
Backstepping control of a doubly-fed induction machine based on fuzzy controller

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RESUME, Ce papier présente la conception d'une nouvelle commande non linéaire pour la machine asynchrone à double alimentation (MADA). La commande proposée est conçue à partir d'une technique de commande de type Backstepping complétée par un contrôleur flou de type 2 pour améliorer sa robustesse. En utilisant la théorie de stabilité de Lyapunov, on montre que les dynamiques de poursuite de trajectoire sont asymptotiquement stables. Afin de simplifier la commande, nous appliquons la commande par orientation du flux statorique qui a l'avantage d'avoir un découplage entre le flux et le courant. Les résultats de simulation montrent la qualité de la commande proposée malgré les incertitudes paramétriques.

Abstract. This paper presents the design of a new nonlinear control for the doubly fed induction machine (DFIM). The proposed control is based on a Backstepping type control technique supplemented by a type 1 fuzzy controller to improve its robustness. Using the Lyapunov stability theory, it is shown that trajectory tracking dynamics are asymptotically stable. In order to simplify the control, we apply the control by orientation of the stator flux which has the advantage of having a decoupling between the flow and the current. The simulation results show the quality of the proposed control despite parametric uncertainties.

Mots-clés : Machine asynchrone à double alimentation, commande backstepping, théorème de Lyapunov, orientation de flux statorique, logique floue, commande hybride, robustesse.

KEYWORDS: Doubly-fed induction machine (DFIM), Backstepping control, Theory of Lyapunov, Stator flux orientation, fuzzy logic, Hybrid control, Robustness.

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1. Introduction

The control of nonlinear systems was of great interest at the end of the 1980s, with the first version of input-output linearization. Later, M. Krstić, and P. V. Kokotović (Krstić M. *and al*, 1995 ; Kokotović P.V., 1992), introduced methods using recursive variable changes called backstepping, on classes of parametric nonlinear triangular systems. In general, the proposed control laws satisfy good properties of robustness and attenuation of disturbances, but only apply to restricted classes of systems and use only static controllers. By introducing a dynamic change of variables and using a Lyapunov function, simple controllers and adaptation laws were obtained for more general classes of nonlinear systems in 1980 (Marce L. *and al*, 1981).

Among the non-linear systems most used in the world of industry is the dual-power asynchronous machine, it is a three-phase asynchronous machine with a wound rotor that can be powered by two voltage sources, one to the stator and the other to the rotor (Vicatos M.S. *and al*, 2003 ; Rouabhi R., 2016). This is due to several factors such as: the quality of robustness, reliability where we mainly appreciate its low maintenance and low cost and very good standardization. The absence of natural decoupling between the inductor and the armature, gives the dual-power asynchronous machine a non-linear dynamic model which is the opposite of the simplicity of its structure. Therefore this order poses a theoretical problem which complicates his model because the parameters of the asynchronous dual feed machine are known approximately and can vary with time (temperature), hence the interest of using the command robust by backstepping.

The backstepping technique has been applied for various electric motors, in particular the doubly-fed induction motor (El Fadili A. *and al*, 2013 ; Tan H. *and al*, 1999 ; Ghanes M. *and al*, 2004). This approach consists in finding a Lyapunov function that allows deducing a control law for the system while showing the overall control stability. On the other hand, the vector control of the asynchronous machine aims to match the performance offered by the control of a separate excitation DC machine. Indeed, in the latter the decoupling between the flux and the torque is naturally achieved which makes these two quantities independently controlled (Ghanes M., 2004).

This work presents the application of the backstepping to the control of the doubly-fed induction machine, based on the principle of the orientation of the stator flux. This approach allows us to determine the components of the machine supply voltages by ensuring the overall stability by Lyapunov's theory. The control thus obtained makes it possible to monitor speed, flux and current, each time ensuring stable dynamics for errors between the reference and actual quantities of speed, flux and current.

In the end, we propose a command based on backstepping and type 1 fuzzy logic to build iteratively and systematically an asymptotically stable robust control law according to the Lyapunov stability theory. This technique consists in replacing the gains of the regulations in the backstepping command by a fuzzy controller of type 1

at an input are the error between the measured value and the reference value. The proposed control technique presents high performance transient and permanent and also vis-à-vis parametric uncertainties.

The rest of this article is organized as follows. Section 2 recalls the mathematical model of the DFIM and the simplified model which has a decoupling between the flow and the current. In the 3 section, we synthesize a backstepping control law of the DFIM. Then section fourth presents a theoretical study on fuzzy logic type 1. Simulation results are presented in the fifth section and conclusions are drawn in the last part of this article.

2. Mathematical modeling of DFIM

The model of the doubly-fed induction machine is expressed in a reference linked to the rotating field (d, q) , the electrical equations of the DFIM write in the form:

$$\begin{cases} V_{sd} = R_s I_{sd} + \frac{d\varphi_{sd}}{dt} - \omega_s \varphi_{sq} \\ V_{sq} = R_s I_{sq} + \frac{d\varphi_{sq}}{dt} + \omega_s \varphi_{sd} \\ V_{rd} = R_r I_{rd} + \frac{d\varphi_{rd}}{dt} - (\omega_s - \omega_r) \varphi_{rq} \\ V_{rq} = R_r I_{rq} + \frac{d\varphi_{rq}}{dt} + (\omega_s - \omega_r) \varphi_{rd} \end{cases} \quad (1)$$

Where:

$$\omega_r = \omega_s - P \cdot \Omega$$

The magnetic equations of the DFIM can be written:

$$\begin{cases} \varphi_{sd} = L_s I_{sd} + M \cdot I_{rd} \\ \varphi_{sq} = L_s I_{sq} + M \cdot I_{rq} \\ \varphi_{rd} = L_r I_{rd} + M \cdot I_{sd} \\ \varphi_{rq} = L_r I_{rq} + M \cdot I_{sq} \end{cases} \quad (2)$$

$L_s = l_s - M_s$ and $L_r = l_r - M_r$: cyclic inductances of a stator and rotor phase ;

$[l_s]$ and $[l_r]$: own inductances of a stator and rotor phase ;

M_s and M_r : mutual inductances between two phases respectively stator and rotor ;

M : maximum mutual inductance between a stator and rotor phase (the axes of the two phases coincide).

The expression of the electromagnetic torque of the DFIM according to the stator flows and currents is written as follows:

$$C_{em} = P \frac{M}{L_s} (\varphi_{sq} I_{rd} - \varphi_{sd} I_{rq}) \quad (3)$$

With P : number of pairs of DFIM poles.

The model of the doubly-fed induction machine can be written in matrix form as follows (Rouabhi R., 2016):

$$\dot{X} = AX + BU \tag{4}$$

Where:

$$X = [\varphi_{sd} \quad \varphi_{sq} \quad I_{rd} \quad I_{rq}]^T \text{ and } U = [V_{sd} \quad V_{sq} \quad V_{rd} \quad V_{rq}]^T$$

$$[A] = \begin{bmatrix} -\frac{1}{T_s} & \omega_s & \frac{M}{T_s} & 0 \\ -\omega_s & -\frac{1}{T_s} & 0 & \frac{M}{T_s} \\ \alpha & -\beta\omega & -\delta & (\omega_s - \omega) \\ \beta\omega & \alpha & -(\omega_s - \omega) & -\delta \end{bmatrix}; [B] = \begin{bmatrix} 1 & 0 & 0 & 0 \\ 0 & 1 & 0 & 0 \\ -\frac{M}{\sigma L_s L_r} & 0 & \frac{1}{\sigma L_r} & 0 \\ 0 & -\frac{M}{\sigma L_s L_r} & 0 & \frac{1}{\sigma L_r} \end{bmatrix}$$

With:

$$\sigma = 1 - \frac{M^2}{L_r L_s}; T_r = \frac{L_r}{R_r}; T_s = \frac{L_s}{R_s}; \alpha = \frac{M}{\sigma L_r L_s T_s}; \beta = \frac{M}{\sigma L_r L_s}; \delta = \frac{1}{\sigma} \left(\frac{1}{T_r} + \frac{M^2}{L_s T_s L_r} \right)$$

The mechanical equation is of the following form:

$$J \frac{d\Omega}{dt} = C_{em} - C_r - f\Omega \tag{5}$$

With:

C_{em} and C_r : the electromagnetic torque and the resisting torque (the mechanical load) ; f and J : coefficient of friction and moment of inertia of the rotor shaft.

In our study, the frequency and the tension are constant. We can see, from relation (3), the strong coupling between flows and currents. Indeed, the electromagnetic torque is the cross product between the flows and the stator currents, which makes the control of the DFIM particularly difficult. In order to simplify the order, we approximate its model to that of the DC machine which has the advantage of having a natural decoupling between the flows and the currents. For this, we apply the flow orientation control which consists in aligning the stator flux φ_s along the d axis of the rotating reference, (Figure 1), (Vidal P.E., 2004 ; Boyette A., 2006). We thus have: $\varphi_{sd} = \varphi_s$ and consequently $\varphi_{sq} = 0$.

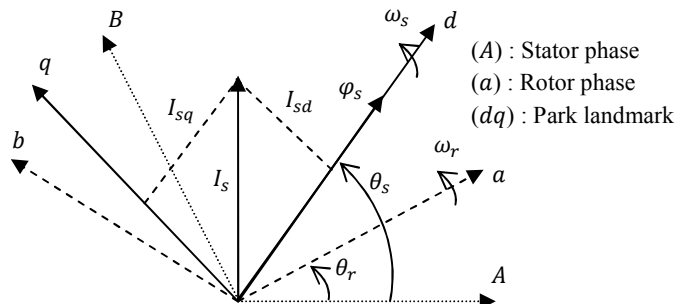


Figure 1. Stator flux orientation on the d axis.

The electromagnetic torque of equation (3) is then written:

$$C_{em} = -P \frac{M}{L_s} \varphi_{sd} I_{rq} \quad (6)$$

And the equation (2) of the flows becomes:

$$\begin{cases} \varphi_{sd} = \varphi_s = L_s I_{sd} + M \cdot I_{rd} \\ \varphi_{sq} = 0 = L_s I_{sq} + M \cdot I_{rq} \end{cases} \quad (7)$$

$$\text{So: } \begin{cases} I_{sd} = \frac{1}{L_s} (\varphi_s - M I_{rd}) \\ I_{sq} = -\frac{1}{L_s} M I_{rq} \end{cases}$$

If one takes the stator current in the axis of null, $I_{sd} = 0$, realistic hypothesis for the machines of high power, the current and the tension in this axis are then in phase $V_s = V_{sq}$ and $I_s = I_{sq}$.

In this case, we get:

$$\begin{cases} I_{rd} = \frac{\varphi_s}{M} \\ I_{rq} = -\frac{L_s}{PM\varphi_s} C_{em} \end{cases} \quad (8)$$

With the assumption of constant stator flux, we obtain the electric equations in the form:

$$\begin{cases} V_{sd} = R_s I_{sd} \\ V_{sq} = R_s I_{sq} + \omega_s \varphi_{sd} \\ V_{rd} = R_r I_{rd} - (\omega_s - \omega_r) \varphi_{rq} \\ V_{rq} = R_r I_{rq} + (\omega_s - \omega_r) \varphi_{rd} \end{cases} \quad (9)$$

In the principle of the orientation of the stator field ($\varphi_{sq} = 0$), the model of the doubly-fed induction machine is written:

$$\begin{cases} \frac{d\varphi_{sd}}{dt} = \frac{M}{T_s} I_{rd} - \frac{1}{T_s} \varphi_{sd} + V_{sd} \\ \frac{d\varphi_{sq}}{dt} = \frac{M}{T_s} I_{rq} - \omega_s \varphi_{sd} + V_{sq} \\ \frac{dI_{rd}}{dt} = -\delta I_{rd} + (\omega_s - \omega) I_{rq} + \alpha \varphi_{sd} - \frac{M}{\sigma L_s L_r} V_{sd} + \frac{1}{\sigma L_r} V_{rd} \\ \frac{dI_{rq}}{dt} = -(\omega_s - \omega) I_{rd} - \delta I_{rq} + \beta \omega \varphi_{sd} - \frac{M}{\sigma L_s L_r} V_{sq} + \frac{1}{\sigma L_r} V_{rq} \end{cases} \quad (10)$$

The mechanical equation is written:

$$\frac{d\Omega}{dt} = -\frac{1}{J} \left(P \frac{M}{L_s} \varphi_{sd} I_{rq} + f\Omega + C_r \right) \quad (11)$$

3. Backstepping control of DFIM

The backstepping control technique is a non-linear synthesis method when it is difficult to apply the direct method of Lyapunov. It is a question of choosing initially a function of Lyapunov for the first subsystem and of increasing it as one stabilizes the various successive subsystems, to finally arrive at a global Lyapunov function which stabilizes the overall system (Tan H. *and al*, 1999 ; Ghanes M. *and al*, 2004 ; Benchaib A., 1998).

The backstepping control of the DFIM consists of the following three steps.

Step 1:

This first step consists in identifying the errors z_1 and z_2 which respectively represent the error between the real speed Ω and the reference speed Ω_{ref} as well as the rotor flow modulus φ_{sd} and the reference one φ_{sd}^{ref} .

$$\begin{aligned} z_1 &= \Omega_{ref} - \Omega \\ z_2 &= \varphi_{sd}^{ref} - \varphi_{sd} \end{aligned} \quad (12)$$

The derivative of the error is given by:

$$\begin{aligned} \dot{z}_1 &= \dot{\Omega}_{ref} - \dot{\Omega} = \dot{\Omega}_{ref} + \frac{1}{J} \left(P \frac{M}{L_s} \varphi_{sd} I_{rq} + f\Omega + C_r \right) \\ \dot{z}_2 &= \dot{\varphi}_{sd}^{ref} - \dot{\varphi}_{sd} = \dot{\varphi}_{sd}^{ref} - \left(\frac{M}{T_s} I_{rd} - \frac{1}{T_s} \varphi_{sd} + V_{sd} \right) \end{aligned} \quad (13)$$

The first function of Lyapunov is defined by:

$$v_1 = \frac{1}{2} (z_1^2 + z_2^2) \quad (14)$$

Then, the derivative of (14) is calculated as:

$$\dot{v}_1 = z_1 \left(\dot{\Omega}_{ref} + \frac{1}{J} \left(P \frac{M}{L_s} \varphi_{sd} I_{rq} + f\Omega + C_r \right) \right) + z_2 \left(\dot{\varphi}_{sd}^{ref} - \left(\frac{M}{T_s} I_{rd} - \frac{1}{T_s} \varphi_{sd} + V_{sd} \right) \right) \quad (15)$$

The stabilizing functions are chosen as follows:

$$\begin{cases} I_{rq}^{ref} = -\frac{JL_s}{pM\varphi_{sd}} \left(k_1 z_1 + \dot{\Omega}_{ref} + \frac{f}{J} \Omega + \frac{C_r}{J} \right) \\ I_{rd}^{ref} = \frac{T_s}{M} \left(k_2 z_2 + \dot{\varphi}_{sd}^{ref} - V_{sd} + \frac{1}{T_s} \varphi_{sd} \right) \end{cases} \quad (16)$$

Where k_1 and k_2 are positive design constants. Then (13) can be expressed as:

$$\begin{aligned} \dot{z}_1 &= -k_1 z_1 \\ \dot{z}_2 &= -k_2 z_2 \end{aligned} \quad (17)$$

The derivative of the function of Lyapunov with respect to time is:

$$\dot{v}_1 = -k_1 z_1^2 - k_2 z_2^2 < 0 \quad (18)$$

Step 2:

In this step, two new errors of the components of the current given by:

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$$\begin{aligned} z_3 &= i_{rq}^{ref} - I_{rq} = -\frac{JL_s}{pM\varphi_{sd}}(k_1 z_1 + u_1) - I_{rq} \\ z_4 &= i_{rd}^{ref} - I_{rd} = \frac{T_s}{M}(k_2 z_2 + u_2) - I_{rd} \end{aligned} \quad (19)$$

Its derivative is given by:

$$\begin{aligned} \dot{z}_3 &= \dot{i}_{rq}^{ref} - \dot{I}_{rq} = \dot{i}_{rq}^{ref} - \left(\eta_1 + \frac{1}{\sigma L_r} V_{rq} \right) \\ \dot{z}_4 &= \dot{i}_{rd}^{ref} - \dot{I}_{rd} = \dot{i}_{rd}^{ref} - \left(\eta_2 + \frac{1}{\sigma L_r} V_{rd} \right) \end{aligned} \quad (20)$$

$$\text{Or : } \begin{cases} \eta_1 = -(\omega_s - \omega)I_{rd} - \delta I_{rq} + \beta \omega \varphi_{sd} - \frac{M}{\sigma L_s L_r} V_{sq} \\ \eta_2 = -\delta I_{rd} + (\omega_s - \omega)I_{rq} + \alpha \varphi_{sd} - \frac{M}{\sigma L_s L_r} V_{sd} \end{cases}$$

Step 3:

To define the control laws, we adopt a new function of lyapunov described by the following expression:

$$v_2 = \frac{1}{2}(z_1^2 + z_2^2 + z_3^2 + z_4^2) \quad (21)$$

So the derivative of the final lyapunov function is:

$$\dot{v}_2 = z_1 \dot{z}_1 + z_2 \dot{z}_2 + z_3 \dot{z}_3 + z_4 \dot{z}_4 \quad (22)$$

This equation can be rewritten in the following from:

$$\dot{v}_2 = z_1 \dot{z}_1 + z_2 \dot{z}_2 + z_3 \left(k_3 z_3 + \dot{i}_{rq}^{ref} - \eta_1 - \frac{1}{\sigma L_r} V_{rq} \right) + z_4 \left(k_4 z_4 + \dot{i}_{rd}^{ref} - \eta_2 - \frac{1}{\sigma L_r} V_{rd} \right) \quad (23)$$

We choose the command as follows:

$$\begin{aligned} V_{rq}^{ref} &= \sigma L_r (k_3 z_3 + \dot{i}_{rq}^{ref} - \eta_1) \\ V_{rd}^{ref} &= \sigma L_r (k_4 z_4 + \dot{i}_{rd}^{ref} - \eta_2) \end{aligned} \quad (24)$$

The choice of $k_3 > 0$ and $k_4 > 0$ can be made such that $\dot{v}_2 < 0$.

Then, (20) can be expressed as:

$$\begin{aligned} \dot{z}_3 &= -k_3 z_3 \\ \dot{z}_4 &= -k_4 z_4 \end{aligned} \quad (25)$$

So from equation (17) and (25) we can write:

$$\dot{v}_2 = -k_1 z_1^2 - k_2 z_2^2 - k_3 z_3^2 - k_4 z_4^2 < 0 \quad (26)$$

4. Fuzzy logic controller

The structure of a complete fuzzy control system is composed from the following blocs: Fuzzification, Knowledge base, Inference engine, Defuzzification. Figure 2 shows the structure of a fuzzy logic controller.

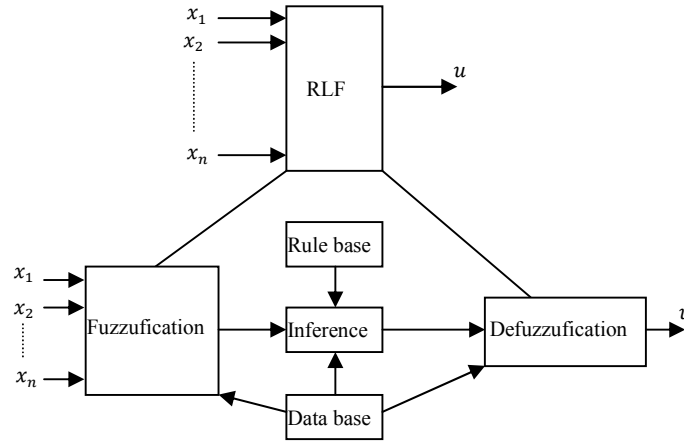


Figure 2. The structure of a fuzzy logic controller.

The fuzzification module converts the crisp values of the control inputs into fuzzy values. A fuzzy variable has values, which are defined by linguistic variables (fuzzy sets or subsets) such as low, medium, high, slow... where each is defined by gradually varying membership function. In fuzzy set terminology, all the possible values that a variable can assume are named universe of discourse, and fuzzy sets (characterized by membership function) cover whole universe of discourse. The shape fuzzy sets can be triangular, trapezoidal, etc (Aissaoui M. *and al*, 2007).

A fuzzy control essentially embeds the intuition and experience of a human operator, and sometimes those of a designer and researcher. The data base and the rules form the knowledge base which is used to obtain the inference relation R. The data base contains a description of input and output variables using fuzzy sets. The rule base is essentially the control strategy of the system. It is usually obtained from expert knowledge or heuristics; it contains a collection of fuzzy conditional statements expressed as a set of IF-THEN rules, such as:

$$R^{(i)}: \text{If } x_1 \text{ is } F_1 \text{ and } x_2 \text{ is } F_2 \dots \text{ and } x_n \text{ is } F_n$$

$$\text{Then } Y \text{ is } G^{(i)}, i = 1, \dots, M \quad (27)$$

Where: (x_1, x_2, \dots, x_n) is the input variables vector, Y is the control variable, M is the number of rules, n is the number fuzzy variables, (F_1, F_2, \dots, F_n) are the fuzzy sets.

For the given rule base of a control system, the fuzzy controller determines the rule base to be fired for the specific input signal condition and then computes the effective control action (the output fuzzy variable) (Aissaoui M. *and al*, 2007 ; Ben Attous D. *and al*, 2010).

The composition operation is the method by which such a control output can be generated using the rule base. Several composition methods, such as max-min or sup-min and max-dot have been proposed in the literature.

The mathematical procedure of converting fuzzy values into crisp values is known as “defuzzification”. A number of defuzzification methods have been suggested. The choice of defuzzification methods usually depends on the application and the available processing power. This operation can be performed by several methods of which center of gravity (or centroid) and height methods are common (Aissaoui M. *and al*, 2007 ; Ben Attous D. *and al*, 2010).

The supervisory type-1 fuzzy of the proposed tuning method contains operators knowledge in the form IF-THEN rules decide the control gains K_i according to the current operating condition of the controlled system. Here, the control rules of the supervisory fuzzy system are developed with the error e and derivative of error e as the premise. And $K_i, i = 1, \dots, 4$ as a consequent of each rules (Amer A. *and al*, 2011 ; Zeglache S. *and al*, 2017).

The general structure of the proposed controller is given in Figure 3.

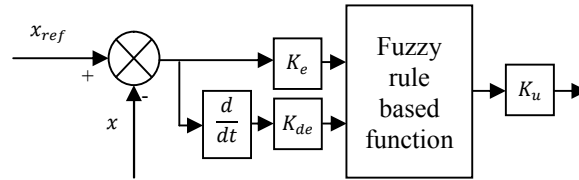


Figure 3. Block diagram of Fuzzy controller.

The membership functions for the inputs and outputs as shown respectively in Fig. 4 and Fig. 5. Fig. 6 shows the type-1 fuzzy control surface of K_i . This surface has been used to adaptively tune $K_i, i = 1, \dots, 4$ on line. The physical domain of the inputs (e, \dot{e}) is in the range $\{-0.01, 0.01\}$ and that of the output K_i is in the range $\{0, 2\}$, respectively, selected based on trial and error approach. The fuzzy variables are defined for the rule base as, $(e, \dot{e}) = \{NB$ (Negative Big), NM (Negative Medium), NS (Negative Small), ZE (Zero), PS (Positive Small), PM (Positive Medium), PB (Positive Big) $\}$; $K_i = \{VVS$ (Very Very Small), VS (Very Small), S (Small), M (Medium), B (Big), VB (Very Big) and VVB (Very Very Big) $\}$. The linguistic fuzzy rules of the supervisory type-1 fuzzy system are given in Table 1.

Table 1. Rule matrix of supervisory type-1 fuzzy control.

K_i		$e(t)$						
		NB	NM	NS	ZE	PS	PM	PB
$\dot{e}(t)$	NB	VVS	VVS	VVS	VVS	M	M	M
	NM	VVS	VVS	VS	VS	M	M	M
	NS	VVS	VVS	S	S	B	B	VB
	ZE	VVS	VS	S	M	B	VB	VVB
	PS	VS	S	S	B	B	VVB	VVB
	PM	M	M	M	VB	VB	VVB	VVB
	PB	M	M	M	VVB	VVB	VVB	VVB

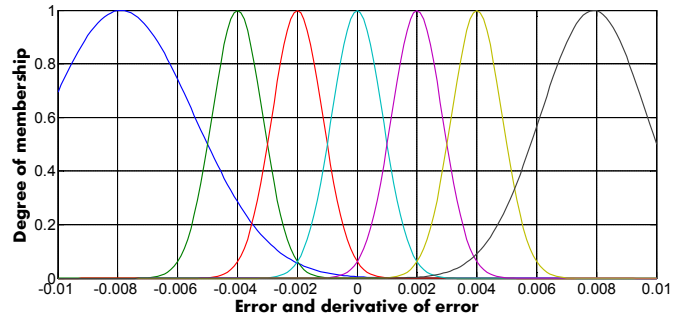


Figure 4. Membership functions for input (e, \dot{e}) .

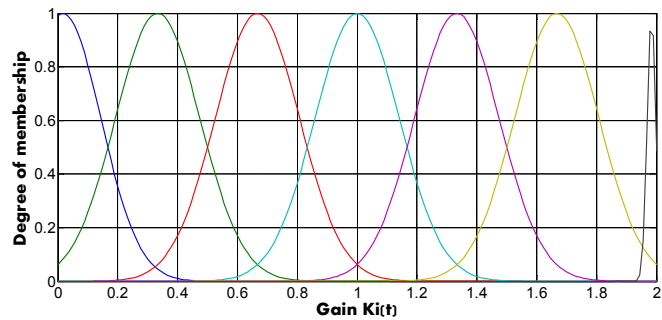


Figure 5. Membership functions for output $K_i(t)$.

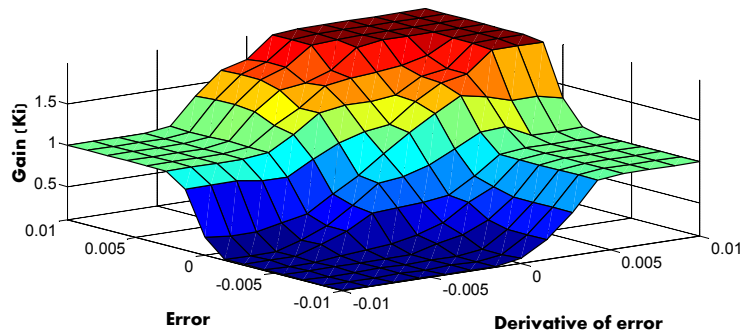


Figure 6. Type-1 fuzzy control of K_i .

The block diagram of the proposed type-1 fuzzy backstepping control scheme is presented in figure 7. The first step of the command is to generate the currents of I_{rq}^{ref} and I_{rd}^{ref} , representing the dummy command. The error between these references and the real quantities of the currents results from new errors z_3 and z_4 . Finally we adapt the control law V_{rq}^{ref} and V_{rd}^{ref} from equation (24) to ensure the stability of the machine.

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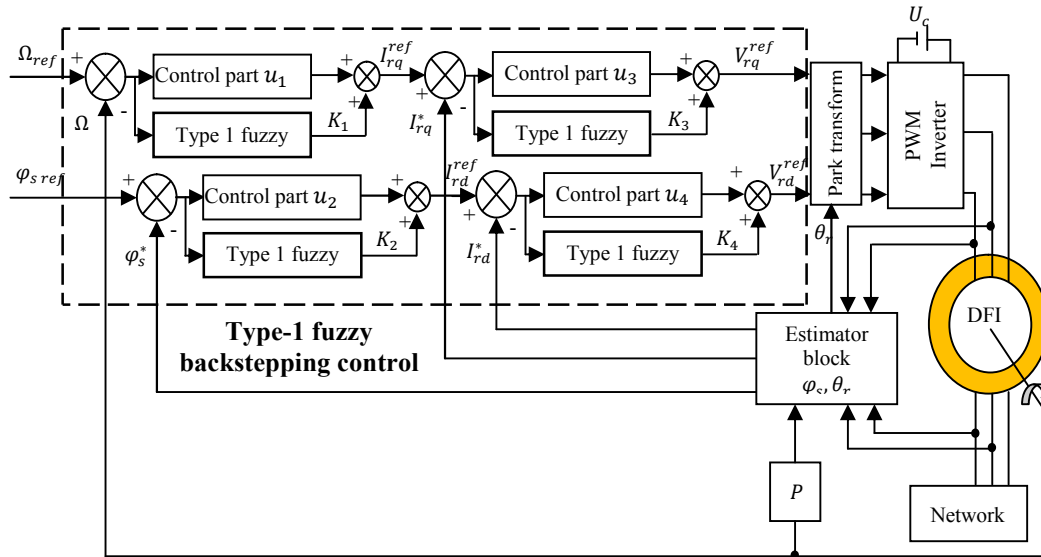
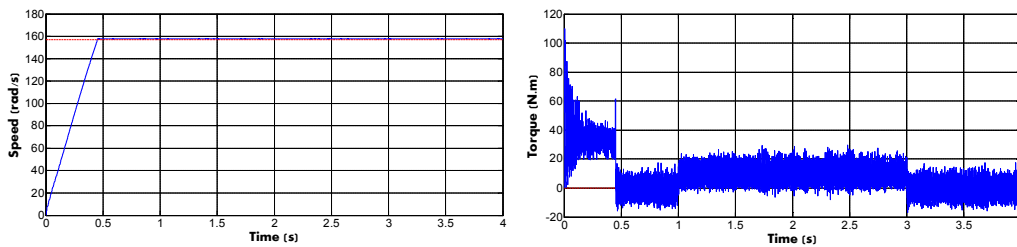


Figure 7. Block diagram of the backstepping control based on fuzzy controller of the DFIM.

5. Simulation results

In this section, simulation results are presented to illustrate the performance and robustness of the proposed control law when applied to the DFIM, which is powered directly by the three-phase network [220/380V, 50Hz] and the rotor is supplied with voltage through a PWM inverter. The parameters of the motor are shown in Appendix.

The simulation results are grouped together in Figure 8. The speed of the machine has a first-order response to the end value of 157 rad/s. Between instants $t = 1$ and $t = 3$ s, a load of value $C_r = 10$ N.m is applied. We find that the load variation does not influence the speed and flux quantities. The principle of vector control is verified by the decoupling between flux and torque.



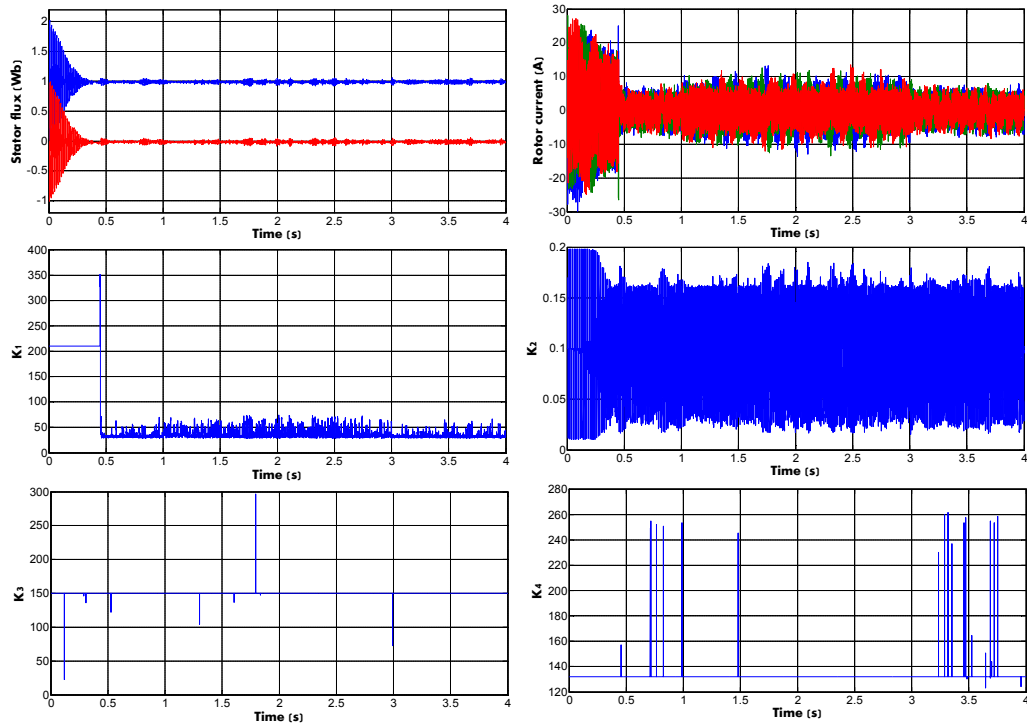
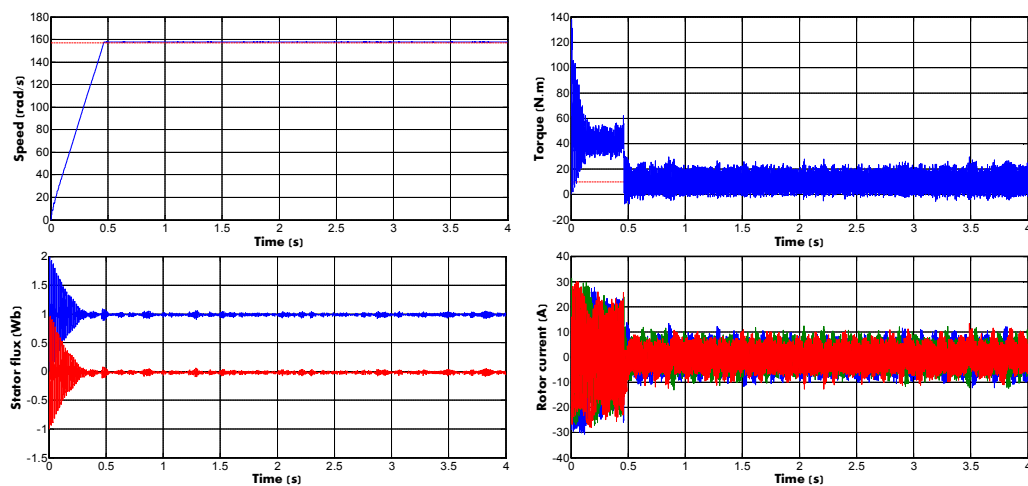


Figure 8. Simulation results of the DFIM controlled by type-1 fuzzy backstepping control.

In the second test a load of value $C_r = 10 \text{ N.m}$ is applied and between instants $t = 1 \text{ s}$ and $t = 3 \text{ s}$ a variation on the rotor resistance at (+50%). The variation of the rotor resistance does not affect the speed and flux quantities. The principle of vector control is always verified.



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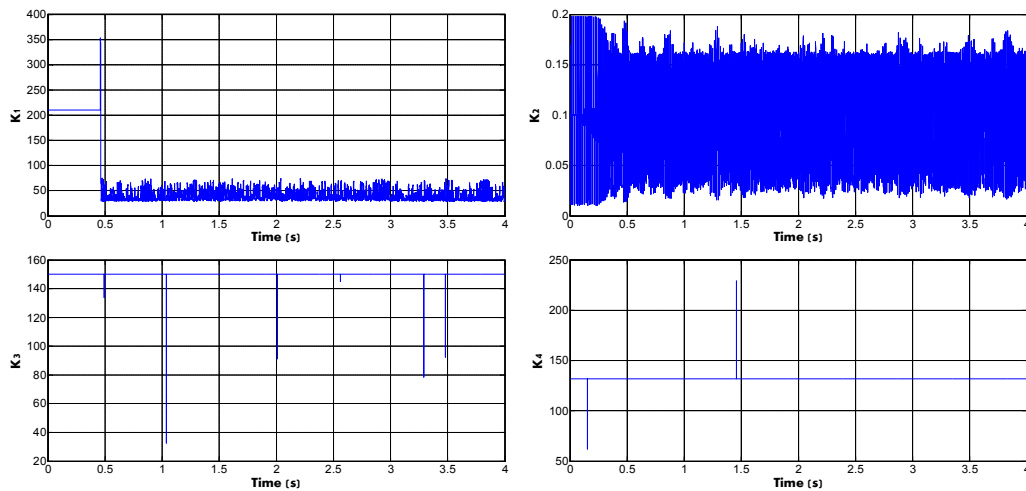


Figure 9. Simulation results of backstepping control of the DFIM based on fuzzy controller with rotor resistance variation (+50%).

6. Conclusion

This paper presents the robust control of the doubly fed induction machine that is based on backstepping control and type 1 fuzzy controller. In this control we have chosen the gains of the regulation by the type 1 fuzzy. After presenting a Mathematical modeling of DFIM, we applied the orientation of stator flux to have the decoupling between the flux and the current for simplified the model of DFIM.

The interest of this command is the robustness; it is to eliminate the effects of the parametric variations even in dynamic regime with a minimum of complexity of the law of control. The structure of this approach is cascaded by backstepping control and fuzzy logic type 1. Simulations results have then shown robustness and good performances when the DFIM is confronted to internal and external perturbations. Furthermore, this regulation presents a simple robust control algorithm.

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Appendix

Table 2. Nomenclature and numeric values of the DFIM (Rouabhi R., 2016).

Parameters	Symbol	Value
Nominal power	P_w	4 KW
Stator voltage	U_{sn}	380 V
Rotor voltage	U_{rn}	220 V
Nominal current	I_n	15/8.6 A
Nominal mechanical speed	Ω_n	1440 rpm
Nominal stator and rotor frequencies	ω_{sn}	50Hz
Pole pair number	P	2
Stator resistance	R_s	1.2 Ω
Rotor resistance	R_r	1.8 Ω
Stator self inductance	L_s	0.1554 H
Rotor self inductance	L_r	0.1568 H
Mutual inductance	M	0.15 H
Moment of inertia	J	0.2 Kg. m ²
Friction coefficient	f	0.001 IS